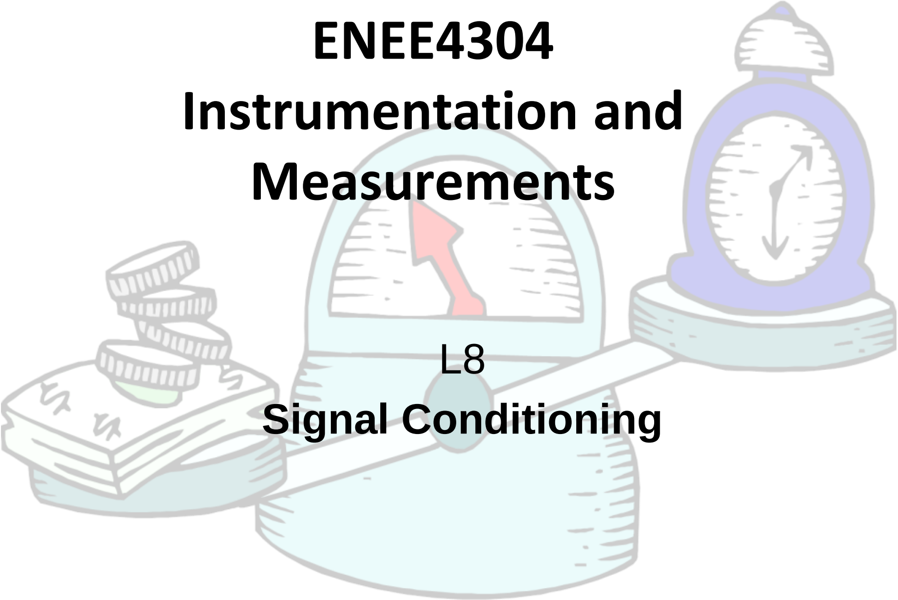


ENEE4304
Instrumentation and Measurements

L8

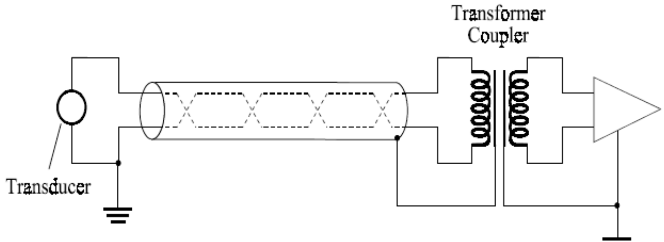
Signal Conditioning

Signal Conditioning Functions

- Isolation
- Filtering
- Amplification
- Linearization (bias removal)
- Excitation

Signal circuit isolation

- Where a signal conductor is required to be earthed/grounded at both ends and additional noise immunity is required, the ground loop should be broken by isolating the signal source from the measuring equipment.
- Isolation by the use of transformers, opto-couplers and common mode chokes, is shown next



Transformer isolation of ground loop

Transformer isolation of ground loop

- When a transformer is used to isolate the signal source from the measurement system the common mode voltage appears between the windings of the transformer and not at the input to the measurement circuit.
- Noise coupling between the circuits is very small and dependent on any stray capacitance between the transformer windings.
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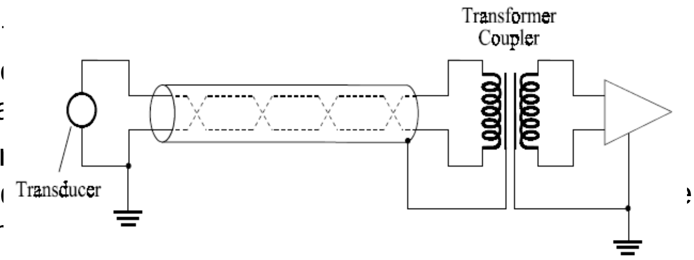
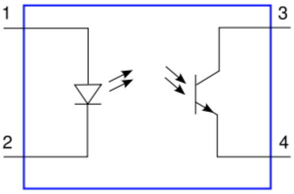
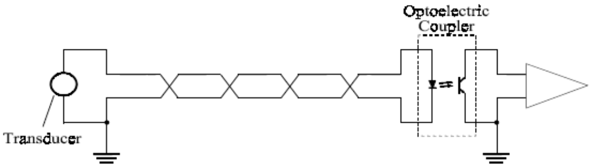


Optocouplers





Optocouplers

- LED for emitter
- Air as barrier for isolation
- Phototransistor for detector

- Transformer is similar, but only for AC
- Optocoupler can be used for DC

When to Use?

- There are many situations where signals and data need to be transferred from one subsystem to another within a piece of electronics equipment, or from one piece of equipment to another, without making a direct electrical connection.
- Often this is because the source and destination are at very different voltage levels, like a microprocessor which is operating from 5V DC but being used to control a triac which is switching 240V AC.
- In such situations the link between the two must be an isolated one, to protect the microprocessor from overvoltage damage.

When to Use?

- ➢ Where small size, higher speed and greater reliability are important, it is much better to use an opto-coupler.
- ➢ These use a beam of light to transmit the signals or data across an electrical barrier, and achieve excellent isolation.

Parameters

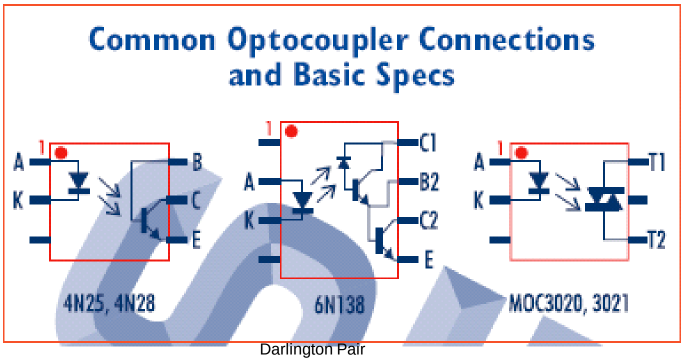
- The most important parameter for optocouplers is their isolation.

- The second most important parameter is transfer efficiency, measured as the current transfer ratio or CTR.
- CTR is simply the ratio between a current change in the output transistor and the current change in the input LED which produced it.
- Typical values for CTR range from 10% to 50% for devices with an output phototransistor and up to 2000% or so for those with a Darlington transistor pair in the output.

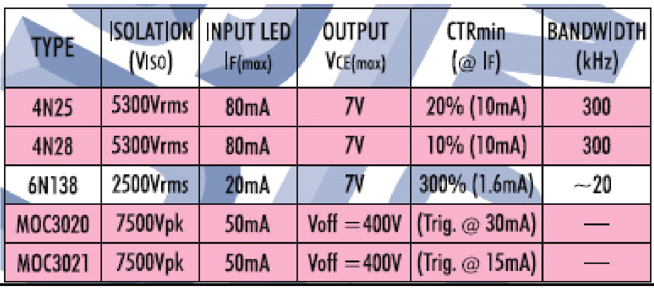
Parameters

- Optocoupler’s bandwidth - determines the highest signal frequency that can be transferred through it
- Typical opto-couplers with a single output phototransistor may have a bandwidth of 200 - 300kHz, while those with a Darlington pair are usually about 10 times lower, at around 20 - 30kHz.

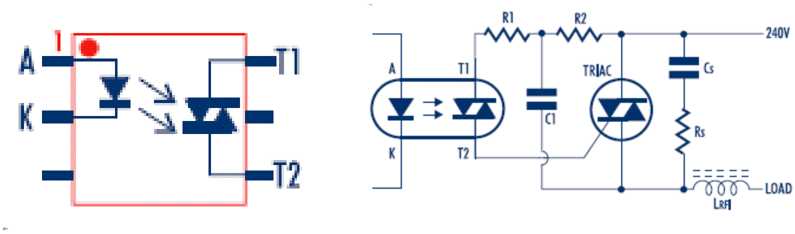
Common Optocoupler Connections and Basic Specs



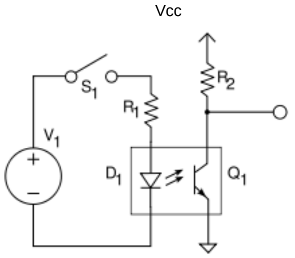
Darlington Pair



TYPE	ISOLATION (V_{ISO})	INPUT LED $I_{F(max)}$	OUTPUT $V_{CE(max)}$	CTRmin (@ I_F)	BANDWIDTH (kHz)
4N25	5300Vrms	80mA	7V	20% (10mA)	300
4N28	5300Vrms	80mA	7V	10% (10mA)	300
6N138	2500Vrms	20mA	7V	300% (1.6mA)	~20
MOC3020	7500Vpk	50mA	Voff = 400V	(Trig. @ 30mA)	—
MOC3021	7500Vpk	50mA	Voff = 400V	(Trig. @ 15mA)	—



- The other main type of optocoupler is the type having an output Diac or bilateral switch, and intended for use in driving a Triac or SCR.
- Examples of these are the MOC3020 and MOC3021.
- Here the output side of the opto-coupler is designed to be connected directly into the triggering circuit of the Triac where it’s operating from and floating at full 120/240 VAC



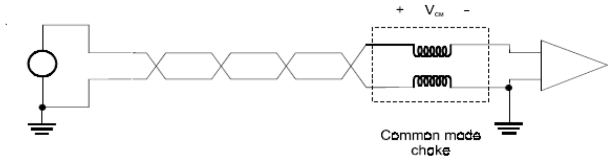
- A simple circuit with an opto-isolator.
- When switch S1 is open, LED D1 is off, so Q1 is off and no current flows through R2, so Vout = Vcc.
- When switch S1 is closed, LED D1 lights.
- Phototransistor Q1 is now triggered, so current flows through R2
- Vout is then pulled down to low state.
- This circuit, thus, acts as a NOT gate.

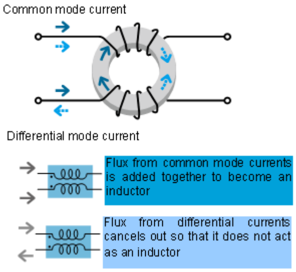
Mechanical Relays

- Mechanical Relays can also provide isolation, but even small relays tend to be fairly bulky compared with ICs.
- Because relays are electro-mechanical, they are not as reliable and are only capable of relatively low speed operation.

Common Mode Choke

- When a transformer is connected as a common mode choke, as shown below
- DC and differential analog signals are transmitted while common mode AC signals are rejected.
- The common mode noise voltage appears across the windings of the choke.
- One big advantage with this type of isolation circuit is that multiple signal circuits can be wound on a common core without coupling.



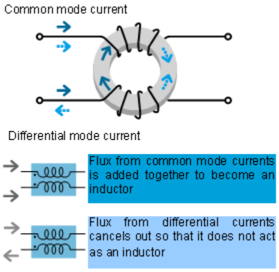


Flux from common mode currents is added together to become an inductor

Flux from differential currents cancels out so that it does not act as an inductor

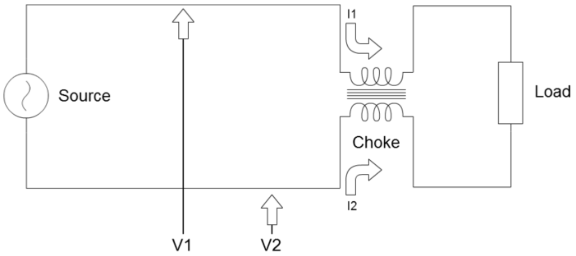
Common-mode choke

- Common-mode chokes, where two coils are wound on a single core, are useful for prevention of electromagnetic interference (EMI) and radio frequency interference (RFI) from power supply lines and for prevention of malfunctioning of electronic equipment.
- They pass differential currents (equal but opposite), while blocking common-mode currents.



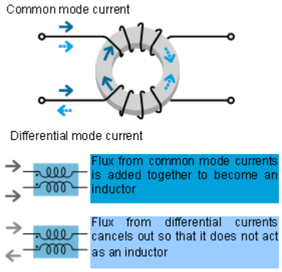
Flux from common mode currents is added together to become an inductor

Flux from differential currents cancels out so that it does not act as an inductor



A typical common-mode choke configuration. The common mode currents, I1 and I2, flowing in the same direction through each of the choke windings, creates equal and in-phase magnetic fields which add together. This results in the choke presenting a high impedance to the common mode signal.

- Magnetic fields produced by differential-mode currents in the windings tend to cancel each other out; thus the choke presents little inductance or impedance to differential-mode currents.
- This also means the core will not saturate even for large differential-mode currents, and the maximum current rating is instead determined by the heating effect of the winding resistance.
- Common-mode currents, however, see a high impedance due to the combined inductance of the windings.



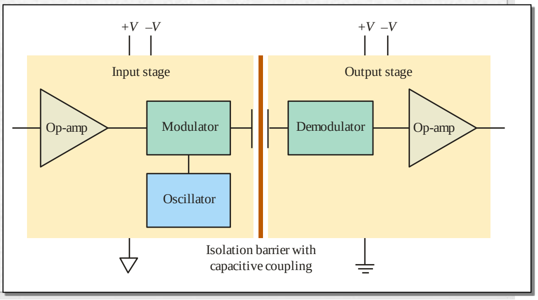
Flux from common mode currents is added together to become an inductor

Flux from differential currents cancels out so that it does not act as an inductor

Isolation Amplifiers

An **isolation amplifier** is designed to provide an electrical barrier between the input and output in order to provide protection in applications where hazardous conditions exist.

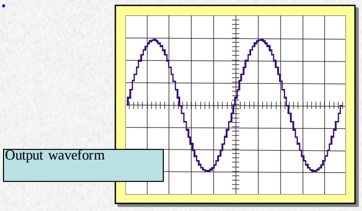
A typical isolation amplifier uses a high frequency modulated carrier frequency to pass a lower frequency signal through the barrier.

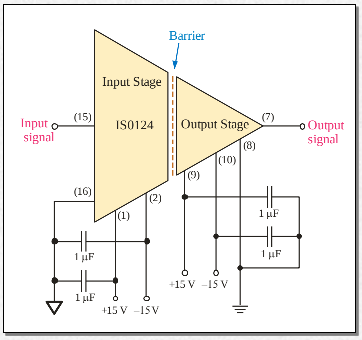


Isolation Amplifiers

The ISO124 is a capacitively-coupled isolation amplifier that uses pulse width modulation to transmit data across the barrier.

The ISO124 has fixed unity gain and is rated to 1500 Vrms of isolation.
The frequency response is specified to 50 kHz, but high-frequency ripple due to the PW modulation may be observed on the output at higher frequencies.

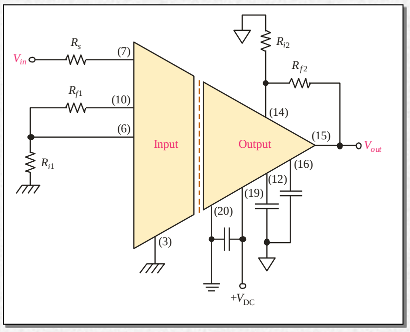




Isolation Amplifiers

The 3656KG is a transformer coupled isolation amplifier that uses pulse width modulation to transmit data across the barrier.

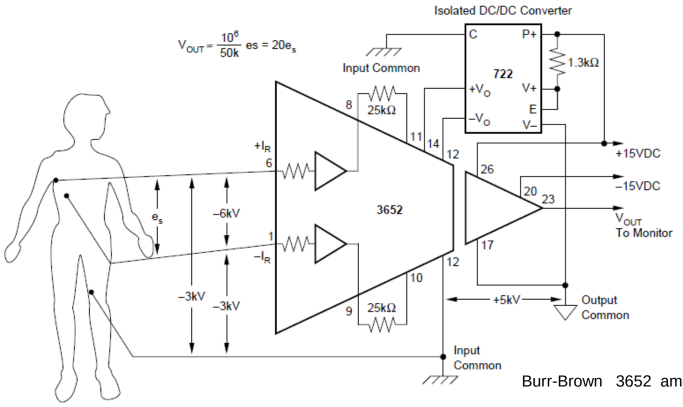
The 3656KG can have gain for both the input and output stages. The 3656KG is suited for patient monitoring applications, such as an ECG amplifier. The manufacture's data sheet shows detailed connection diagrams for various applications1.



1see : http://focus.ti.com/lit/ds/symlink/3656.pdf

Isolation Amplifier

- Mandatory for use in medical equipment to isolate patients body connected electrodes from the equipment grounds



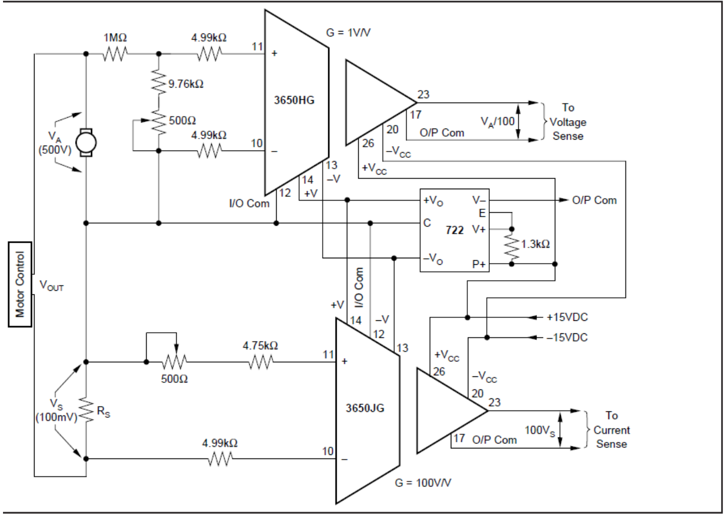
Burr-Brown 3652 amplifier

Isolation Amplifier

- Isolated current & voltage sensor

APPLICATIONS

- INDUSTRIAL PROCESS CONTROL
- DATA ACQUISITION
- INTERFACE ELEMENT
- BIOMEDICAL MEASUREMENTS
- PATIENT MONITORING
- TEST EQUIPMENT
- CURRENT SHUNT MEASUREMENT
- GROUND-LOOP ELIMINATION
- SCR CONTROLS



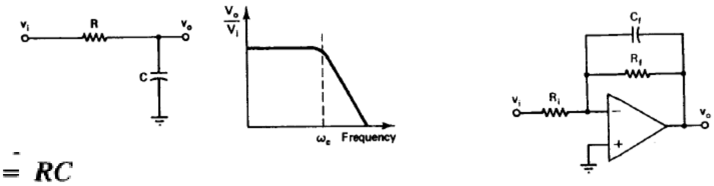
. Isolated Armature Current and Voltage Sensor.

Filtering

- Processing of signal to remove certain band of frequencies from it
- Filters can be classified as : low pass (LPF), high pass (HPF), band-pass (BPF) , band stop (BSF)
- Also filters can be classifiesd as:
  - passive (contain R,L, C)
  - Active (opamp , R,C)

Reminder

- 1^{st} order LPF



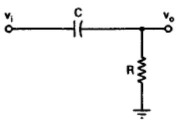
$$\tau = RC$$

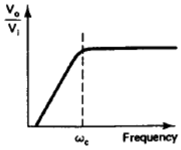
$$\omega_c = 1/\tau$$

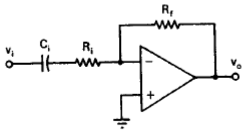
$$\frac{V_o}{V_i} = \frac{1}{1 + j\omega\tau}$$

$$\phi = \tan^{-1}(-\omega\tau)$$

- 1st order HPF



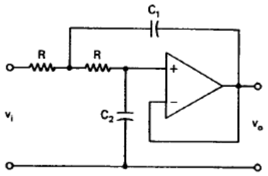


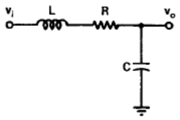


$$\frac{V_o}{V_i} = \frac{j\omega\tau}{1 + j\omega\tau}$$

$$\phi = \tan^{-1}(1/\omega\tau)$$

- 2nd order LPF

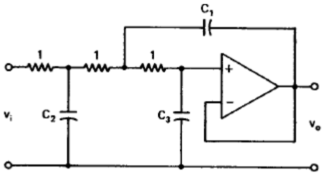




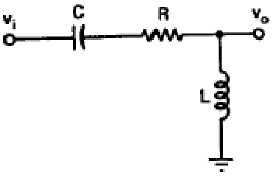
$$\frac{V_o}{V_i} = \frac{1}{(j\omega/\omega_c)^2 + (2\,\zeta\, j\omega/\omega_c) + 1}$$

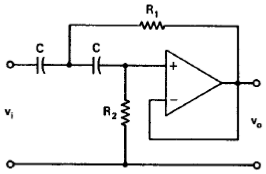
$$\zeta = (R/2)(C/L)^{1/2}$$

$$Q = 1/(2\zeta) = \omega_c/\Delta\omega,$$

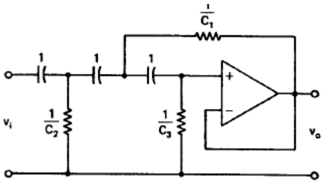


- 2nd order HPF





Second order HPF filter



Normalized third order HPF filter

Op-amp Considerations for active filters

- In most cases we have assumed an ideal op-amp, now we consider some non-ideal characteristics:
- The Gain Bandwidth Product
- Input Offset Voltage
- Slew Rate

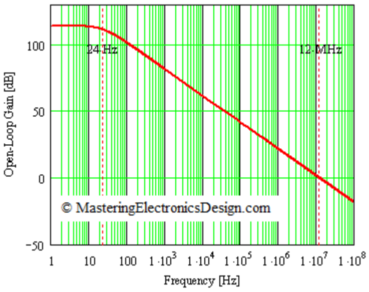
Op-amp Considerations

- The Gain Bandwidth Product describes the op amp gain behavior with frequency.
- Manufacturers insert a dominant pole in the op amp frequency response, so that the output voltage versus frequency is predictable.
- Why do they do that?
- Because the operational amplifier, which is grown on a silicon die, has many active components, each one with its own cutoff frequency and frequency response.
- Because of that, the operational amplifier frequency response would be random, with poles and zeros which would differ from op amp to op amp even in the same family.
- As a consequence, manufacturers thought of introducing a dominant pole in the schematic, so that the op amp response becomes more predictable.
- It is a way of “standardizing” the op amp frequency response. At the same time, it makes the op amp more user friendly, because its stability in a schematic becomes more predictable.

Gain Bandwidth Product (GBW)

- GBW product of an opamp is equal to the product of gain and bandwidth at a particular frequency.
- The gain bandwidth product is constant , thus for a non-inverting amplifier circuit, we obtain the bandwidth by dividing the GBW product by the amplifier circuit gain

$$\text{Bandwidth [Hz]} = \frac{\text{Gain Bandwidth Product [Hz]}}{\text{Closed Loop Gain}}$$

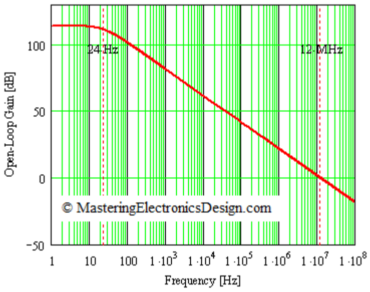


- The dominant pole will make the op amp behave like a single-pole system, which has a drop of 20 dB for every decade of frequency, starting with the cutoff frequency

Gain Bandwidth Product (GBW)

- In the case of ADA4004, the gain bandwidth product is 12 MHz.
- This means that, at a gain of one, the bandwidth is 12 MHz, and at the maximum open-loop gain of 500000, the bandwidth is 12 MHz divided by 500000, which is 24 Hz. This is the op amp open-loop cutoff frequency.

$$\text{Bandwidth [Hz]} = \frac{\text{Gain Bandwidth Product [Hz]}}{\text{Closed Loop Gain}}$$



Input Offset Voltage

- Ideal opamp has the property of zero output voltage when the input voltage is zero
- Practical opamps exhibit this feature; they have an input offset voltage.
- **The input offset voltage is the voltage that must be applied between the input terminals to get zero output**
- The offset voltage is not important when dealing with voltages above 1 V
- The offset voltage is nulled by introducing an opposing voltage at one of the opamp terminals according to data sheet of particular opamp.

Input Bias Current

- In practical opamps, the current flowing into the terminals is not zero
- In order to keep the input transistor of the opamp on, a base or gate current called input bias current is required all the time
- When this current flows through the feedback network it causes errors
- To minimize these errors, feedback resistors should be kept low such as below 10K
- **The effect of bias currents is reduced or eliminated by making the impedances seen by each input of the opamp almost equal**

Slew Rate

- **Slew Rate (SR) is the maximum rate of change of amplifier output voltage**
- When rapid changes are demanded in the output, the current available to charge and discharge the compensation cap is limited and slew rate limiting occurs, for example a 741 opamp has SR of 0.5V/uS
- Thus the output cannot change from -5V to +5V in less than 20 us

Slew Rate (SR)

Slew rate (SR) is the maximum rate at which an op-amp can change output without distortion.

$$SR = \frac{\Delta V_o}{\Delta t} \quad (\text{in } V/\mu s)$$

The SR rating is given in the specification sheets as V/µs rating.

Maximum Signal Frequency

The slew rate determines the highest frequency of the op-amp without distortion.

$$f \le \frac{SR}{2\pi V_p}$$

where V_P is the peak voltage

Power Supply

Power Supply

The usual supply voltages are ±15 V. When v_o is allowed to exceed the op-amp biasing voltages the op amp will saturate and is said to be out of the amplifier's linear range (typically ±13 V). We may reduce the power-supply voltage, but this also reduces the linear range. When the power supply goes below approximately 4 V the internal biasing voltages of the device are not satisfied.

It would be convenient always to have dual-polarity power supplies available in equipment or circuits using op amps. Unfortunately, this is not possible. There are, however, certain circuitry tactics for using the operational amplifier in single-polarity configurations. One solution is to ground the minus supply terminal, while the positive is connected to V_{cc} in the usual way. Figure 1.17 shows this circuit. The noninverting input is connected to a junction on a voltage-divider network. This effectively raises the operating point above ground.

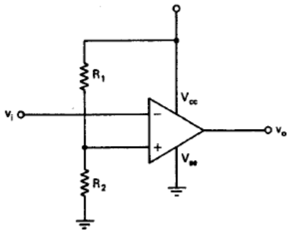


Figure 1.17 Single power-supply circuit.

Different Op Amps

Op amps are bipolar or FET types. The bipolar op amps have a pair of bipolar input transistors. They have good input offset voltage stability but moderate input bias currents and input resistances. FET-input op amps with a pair of input FETs offer very low input bias currents and very high input resistances but have poor input offset voltage stability (Dostal, 1981).

Programmable Op Amps

A programmable op amp such as the UC4250 permits setting the power consumption and dynamic properties of the op amp. By adding the proper external resistor, we can adjust the quiescent supply current [the operating current flowing in a circuit during zero-signal (idle) intervals]. Lower quiescent currents yield lower frequency responses and lower output current capabilities (Dostal, 1981).

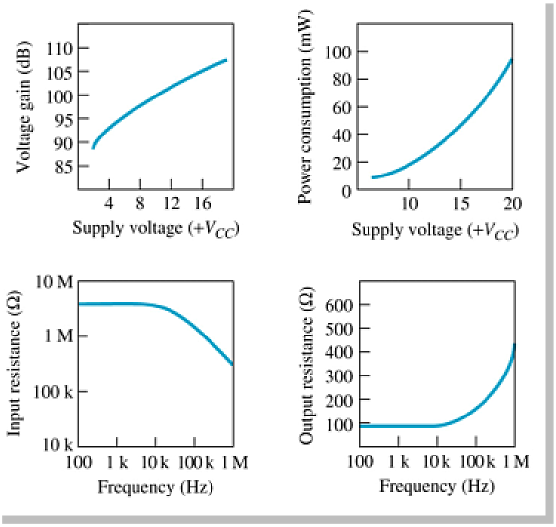
Common opamps

Type	Feature	Input bias current	Offset voltage	GBW	Price
741	Low cost	80 nA	2 mV	1 MHz	$0.35
308	Low bias current	3 nA	2 mV	1 MHz	0.69
ICL8007	FET input	50 pA	50 mV	1 MHz	5.00
CA3130	FET input	6 pA	20 mV	4 MHz	0.89
OP-07	Low offset	1 nA	30 μV	800 kHz	1.99
LH0052	Low offset	0.5 pA	0.1 μV	1 MHz	5.00
LF351	High GBW	50 pA	5 mV	4 MHz	0.62
LM312	Low bias current	3 nA	0.7 mV	1 MHz	2.49
UC4250	Programmable	7.5 nA	4 mV	800 kHz	1.84

	Iomax	funity	slew rate (V/uS)
	mA	MHz	(V/uS)
LF353	20	4	13
LF356	20	5	12
LM318	21	15	70
LM739	1.5	6	1
NE531	20	1	35
TL072	10	3	13
LM741	25	1	0.5
TL074	17	4	13

Op-Amp Performance

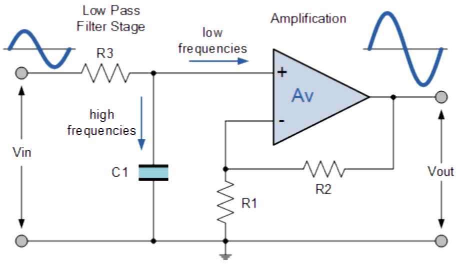
The specification sheets will also include graphs that indicate the performance of the op-amp over a wide range of conditions.



- Design a 1^{st} order LPF for the audio frequency (< 20 kHz) and a dc gain =11 using a LM741C opamp with GBW=1Mhz, SR=0.5 V/us , input impedance 3 Mohm
- What is peak value of output the voltage that can be obtained considering the SR?

Example solution

- Dc gain k= 1+R2/R1=11 ==> R2/R1=10
- Choose R1=5kΩ, ==> R2=50 kΩ
- For balance of resistance at both opamp terminals choose R3=R1//R2
- R3=5k//50k=4.55kΩ
- fc=20 kHz=1/(2πR3C1)
- ==> C1=1.75 nF



- Now assuming Vo=Vp sinωt
- And we can find the ΔV/Δt= ωVp cosωt or slow rate as the max value of ΔV/Δt which is equal to : SR= ωVp =2πf Vp
- and the max allowable values of Vi and Vo are

$$V_{op} \le \frac{SR}{2\pi f}$$

$$V_{op} \le \frac{0.5\ V/\mu sec}{2\pi(20000)Hz} = 3.98\ V$$

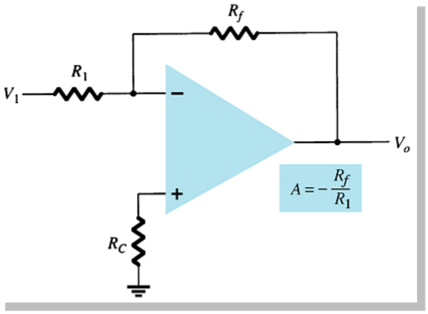
$$Vi(peak) \le \frac{3.98}{11} = 0.362\ V$$

Amplification & other Functions

- Non Inverting amplifier
- Inverting amplifier
- Difference amplifier
- Instrumentation amplifier
- Integrator
- Differentiator
- Log amplifier
- Anti-log amplifier
- Trans-conductance Amplifier
- Rectifiers

Constant-Gain Inverting Amplifier

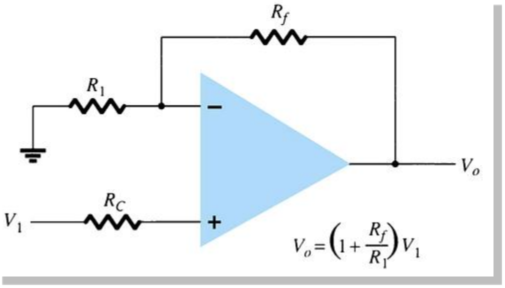
Inverting Version



more…

Noninverting Amplifier Version

The output voltage is the gain times the input voltage. What makes an op-amp different from other amplifiers is its impedance characteristics and gain calculations that depend solely on external resistors.

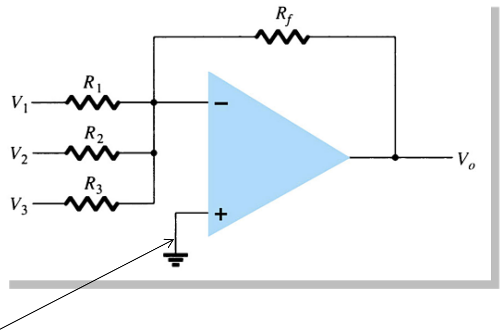


more…

Voltage Summing

The output is the sum of individual signals times the gain:

$$V_o = -\left(\frac{R_f}{R_1}V_1 + \frac{R_f}{R_2}V_2 + \frac{R_f}{R_3}V_3\right)$$



Add resistance equal

=R1//R2//R3//Rf

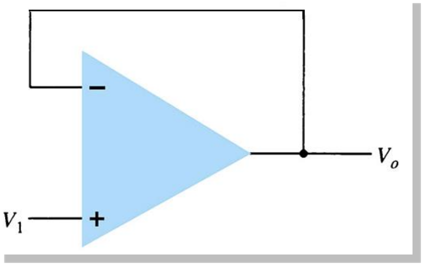
[Formula 14.3]

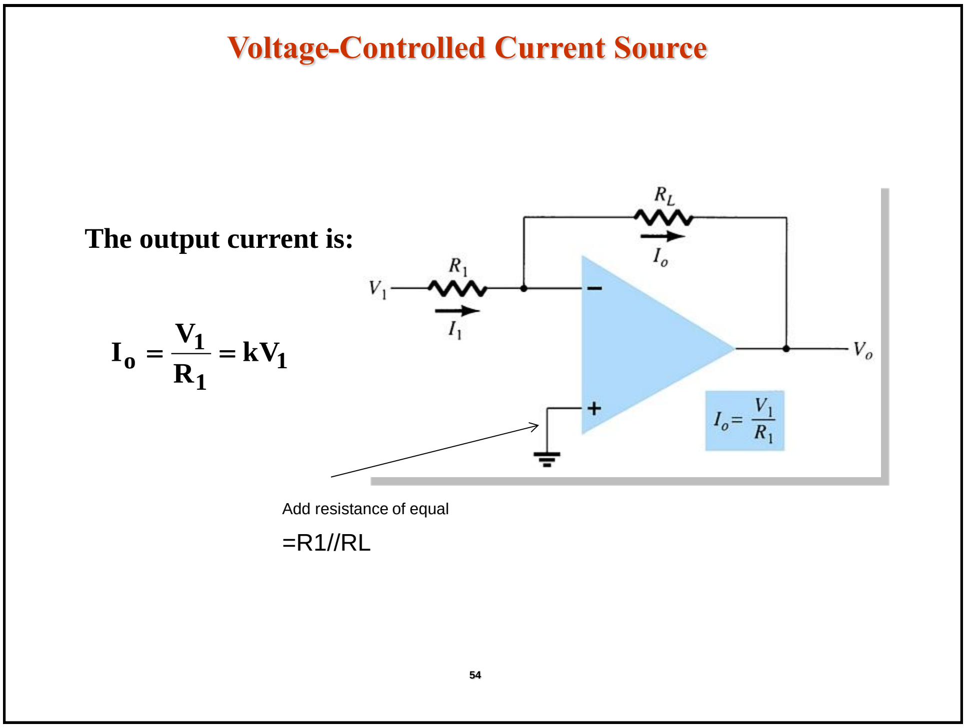
Voltage Buffer

Any amplifier with no gain or loss is called a **unity gain amplifier**.
The advantages of using a unity gain amplifier:

- Very high input impedance
- Very low output impedance

Realistically these circuits are designed using equal resistors ($R_1 = R_f$) to avoid problems with offset voltages.





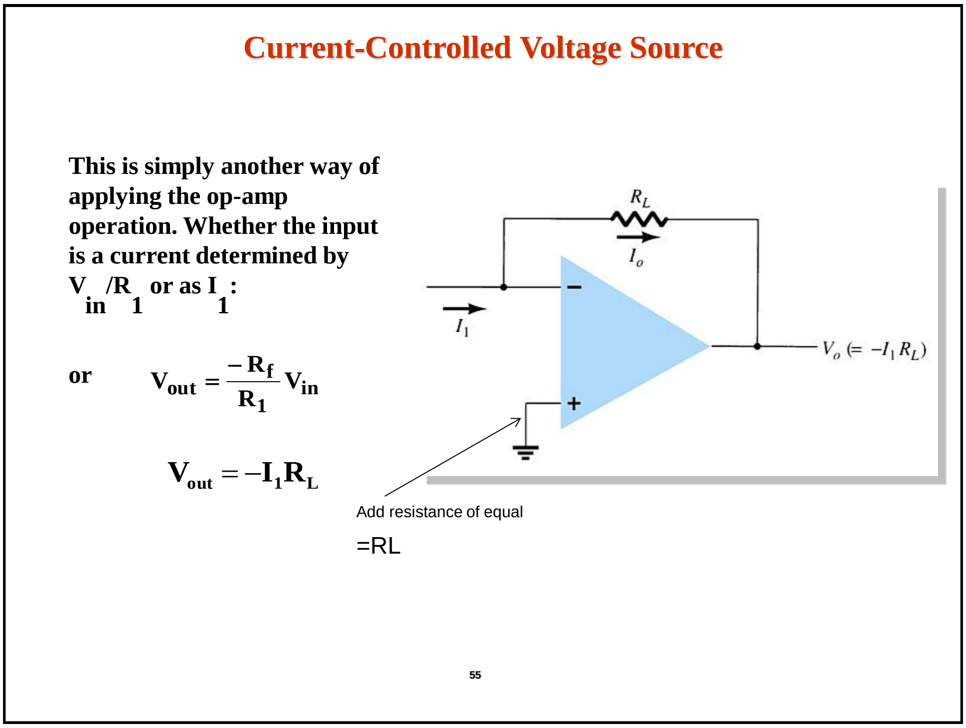
Voltage-Controlled Current Source

The output current is:

$$I_o = \frac{V_1}{R_1} = kV_1$$

Add resistance of equal

=R1//RL



Current-Controlled Voltage Source

This is simply another way of applying the op-amp operation. Whether the input is a current determined by V_{in}/R_1 or as I_1:

or $$V_{out} = \frac{-R_f}{R_1} V_{in}$$

$$V_{out} = -I_1 R_L$$

Add resistance of equal

=RL

Difference Amplifier

$$V_{out} = aV_1 - bV_2$$

$$a = \left(1 + \frac{R_4}{R_2}\right) * \frac{R_3}{R_3 + R_1} = \left(\frac{R_2 + R_4}{R_2}\right) * \frac{R_3}{R_3 + R_1}$$

$$b = \frac{R_4}{R_2}$$

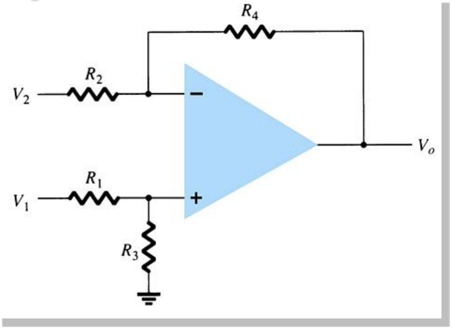
for

$$R4 = R3 = mR$$

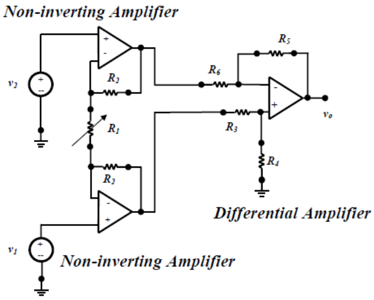
$$R1 = R2 = R$$

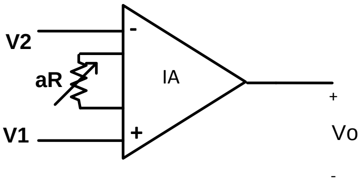
$$\& \, a = b = m$$

$$V_{out} = m(V_1 - V_2)$$



IA





$$Vo = \left(1 + \frac{2}{a}\right)(V_1 - V_2)$$

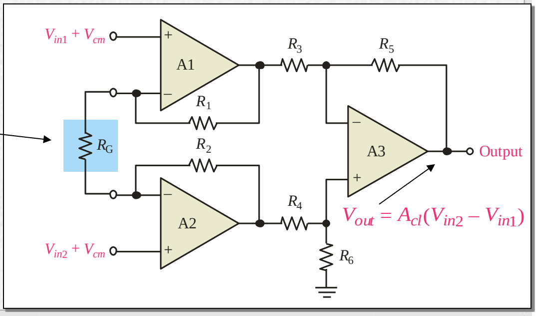
Signal Conditioning

Instrumentation Amplifiers

An **instrumentation amplifier** (IA) amplifies the voltage difference between its terminals. It is optimized for small differential signals that may be riding on a large common mode voltages.

The gain is set by a single resistor that is supplied by the user.

The output voltage is the closed loop gain set by R_G multiplied by the voltage difference in the inputs.



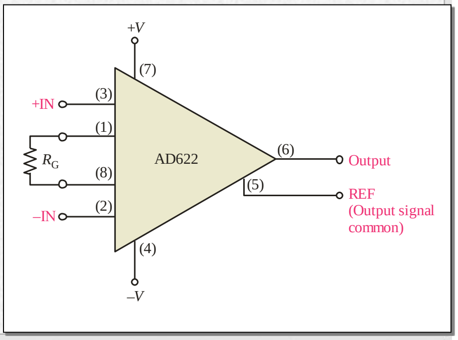
$V_{out} = A_{cl}(V_{in2} - V_{in1})$

Signal Conditioning

Instrumentation Amplifiers

An IA that is based on the three op-amp design is the AD622. The formula for choosing R_G is:

$$R_G = \frac{50.5\ \text{k}\Omega}{A_v - 1}$$



Example: What value of R_G will set the gain to 35?

Solution:

$$R_G = \frac{50.5\ \text{k}\Omega}{A_v - 1} = \frac{50.5\ \text{k}\Omega}{35 - 1}$$

$= 1.5\ \text{k}\Omega$

Signal Conditioning

Instrumentation Amplifiers

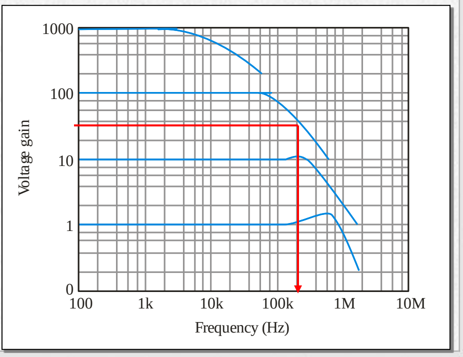
The bandwidth of any IA (or op-amp for that matter) is lower for higher gain. The graph shows the *BW* for various gains for the AD622.

Question:

What is the *BW* for a gain of 35?

Answer:

Reading the graph, the *BW* is approximately 200 kHz.

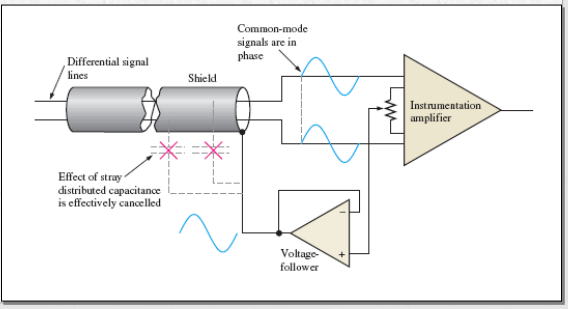


Signal Conditioning

Instrumentation Amplifiers

Guarding is available in some IAs to reduce noise effects. By driving the shield with the common-mode signal, effects of stray capacitance are effectively cancelled.

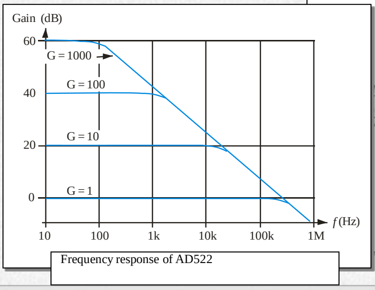
Guarding is useful in applications such as transducer interfacing, and microphone preamps where very small signals need to be transmitted.



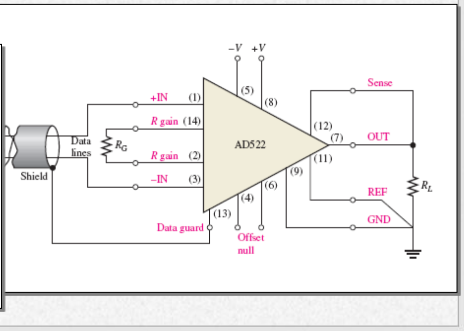
Signal Conditioning

Instrumentation Amplifiers

The AD522 is a low-noise IA that has a *Data guard* output, which is connected to the shield as shown. The AD522 has a programmed gain from 1 to 1000 depending on R_G. The frequency response rolls off at –20 dB/decade.



Frequency response of AD522



Summary

The Operational Transconductance Amplifier

The **operational transconductance amplifier** (OTA) is a voltage-to-current amplifier. As in the case of FETs, the conductance is output current divided by input voltage. Thus,

$$g_m = \frac{I_{out}}{V_{in}}$$

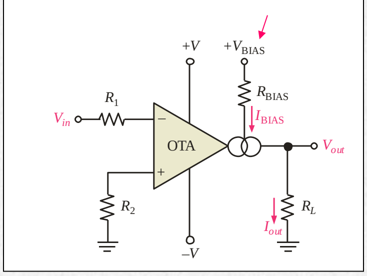
Like FETs, the gain of an amplifier is written in terms of g_m:

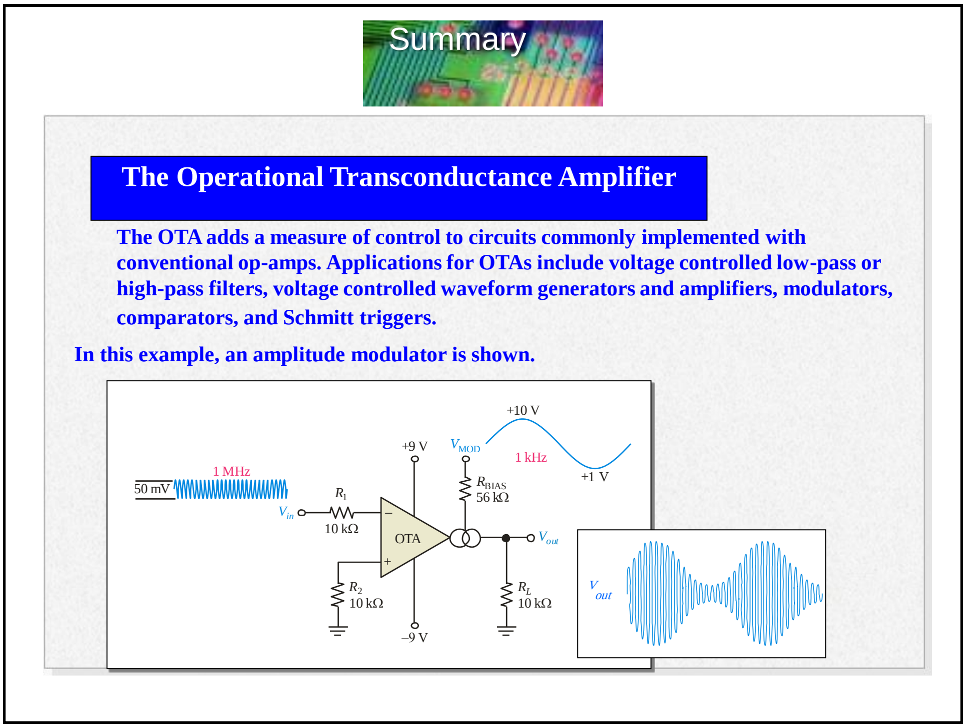
$$A_v = g_m R_L$$

Unlike FETs, the OTA has a g_m that can be "programmed" by the amount of bias current.

Thus gain can be changed electronically by varying a dc voltage.

The gain is controlled by V_{BIAS} in this circuit.



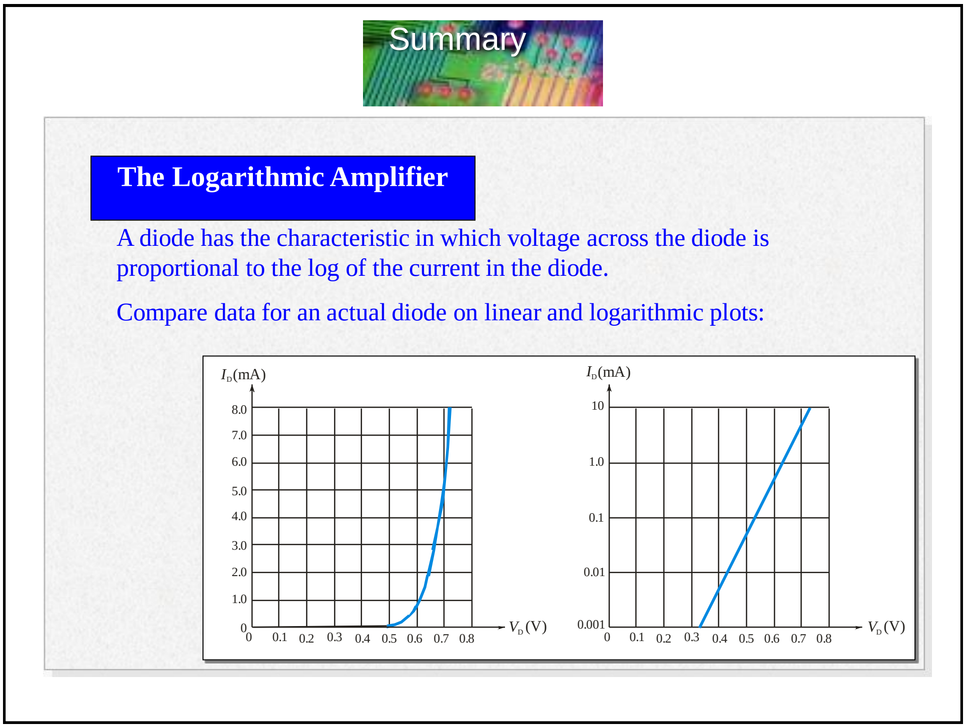


Summary

The Operational Transconductance Amplifier

The OTA adds a measure of control to circuits commonly implemented with conventional op-amps. Applications for OTAs include voltage controlled low-pass or high-pass filters, voltage controlled waveform generators and amplifiers, modulators, comparators, and Schmitt triggers.

In this example, an amplitude modulator is shown.



Summary

The Logarithmic Amplifier

A diode has the characteristic in which voltage across the diode is proportional to the log of the current in the diode.

Compare data for an actual diode on linear and logarithmic plots:

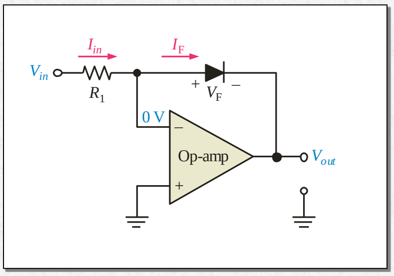
Summary

The Logarithmic Amplifier

When a diode is placed in the feedback path of an inverting op-amp, the output voltage is proportional to the log of the input voltage. The gain decreases with increasing input voltage; therefore the amplifier is said to compress signals.

Many sensors, particularly photo-sensors, have a very large dynamic range outputs.

Current from photodiodes can range over 5 decades. A log amp will amplify the small current more than the larger current to effectively compress the data for further processing.



Summary

The Logarithmic Amplifier

For the circuit shown, the equation for V_{out} is

$$V_{out} \cong -(0.025\text{ V})\ln\frac{V_{in}}{I_R R_1}$$

(I_R is a constant for a given diode.)

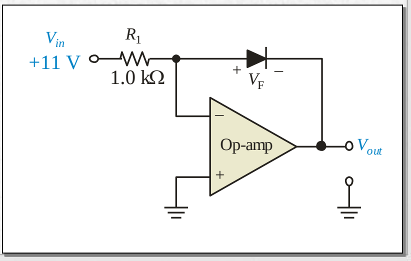
Example:

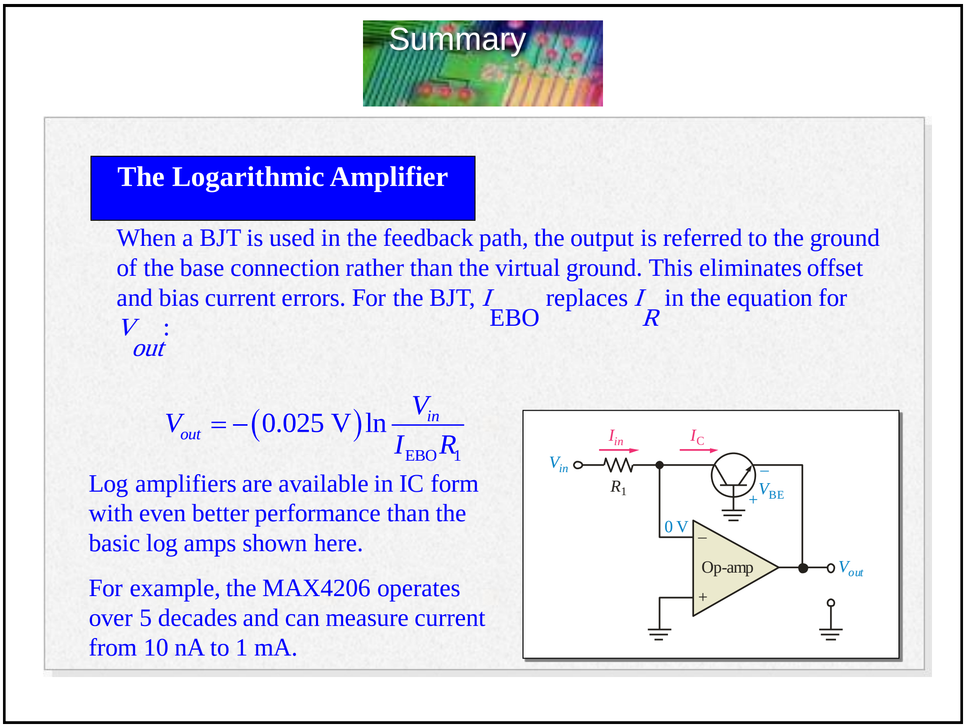
What is V_{out}? (Assume I_R = 50 nA.)

Solution:

$$V_{out} \cong -(0.025\text{ V})\ln\frac{11\text{ V}}{(50\text{ nA})(1.0\text{ k}\Omega)}$$

$= -307$ mV





Summary

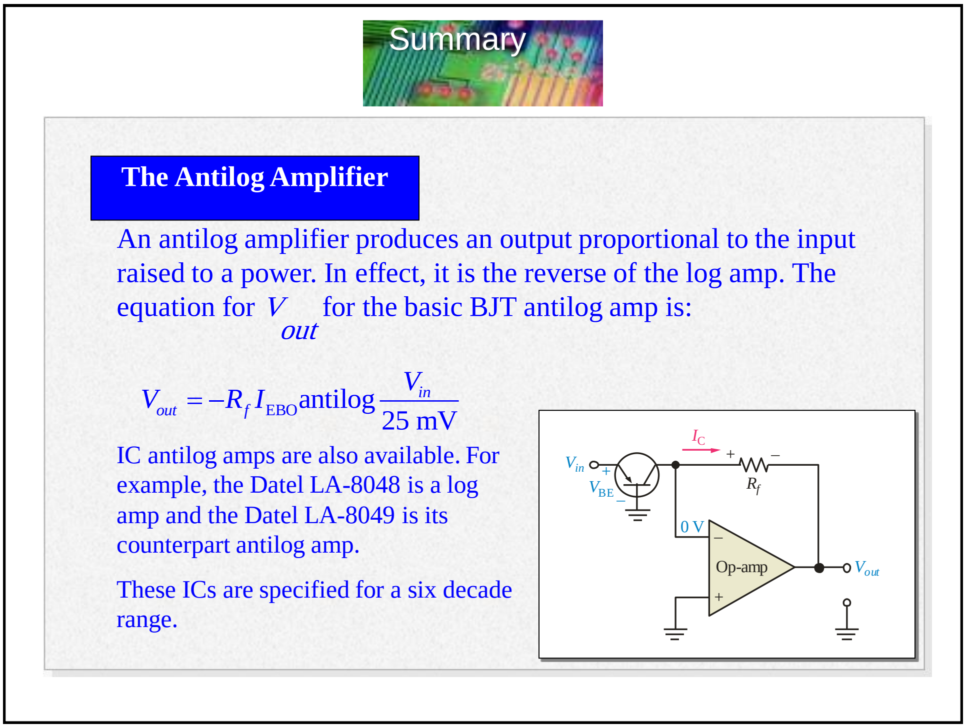
The Logarithmic Amplifier

When a BJT is used in the feedback path, the output is referred to the ground of the base connection rather than the virtual ground. This eliminates offset and bias current errors. For the BJT, I_{EBO} replaces I_R in the equation for V_{out}:

$$V_{out} = -(0.025\text{ V})\ln\frac{V_{in}}{I_{EBO}R_1}$$

Log amplifiers are available in IC form with even better performance than the basic log amps shown here.

For example, the MAX4206 operates over 5 decades and can measure current from 10 nA to 1 mA.



Summary

The Antilog Amplifier

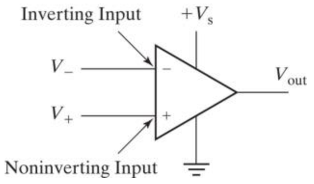
An antilog amplifier produces an output proportional to the input raised to a power. In effect, it is the reverse of the log amp. The equation for V_{out} for the basic BJT antilog amp is:

$$V_{out} = -R_f I_{EBO}\,\text{antilog}\frac{V_{in}}{25\text{ mV}}$$

IC antilog amps are also available. For example, the Datel LA-8048 is a log amp and the Datel LA-8049 is its counterpart antilog amp.

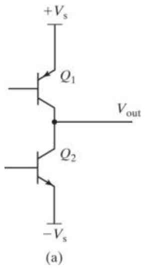
These ICs are specified for a six decade range.

The Comparator

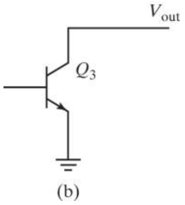


- A specially designed op-amp, optimized to switch V_{out} *fast*
  - If V+ > V-, then $V_{out} \approx$ Vs
  - If V- > V+, then $V_{out} \approx$ 0 V
- But usually output is '*open collector*'
  - Can pull *low*, but…
  - Needs external resistor (pull-up) to go high

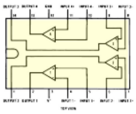
Typical op-amp output stage and *some* comparators (Push-Pull (Totem Pole))



<u>Open collector</u> output stage (typical of most comparators, such as LM339)

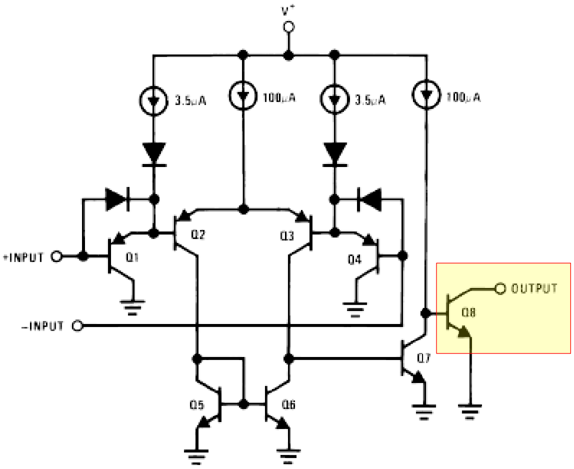


LM339 Quad IC



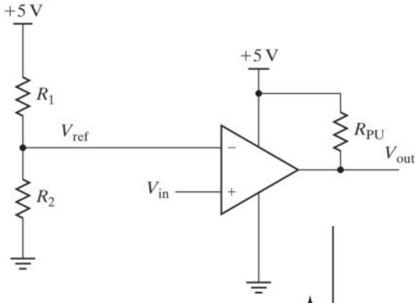
http://www.ermicro.com/blog/?p=1578

Inside the LM339 comparator

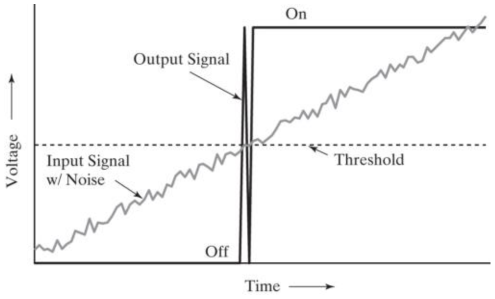


www.national.com/ds/LM/**LM339**.pdf

Simple Non-inverting Comparator

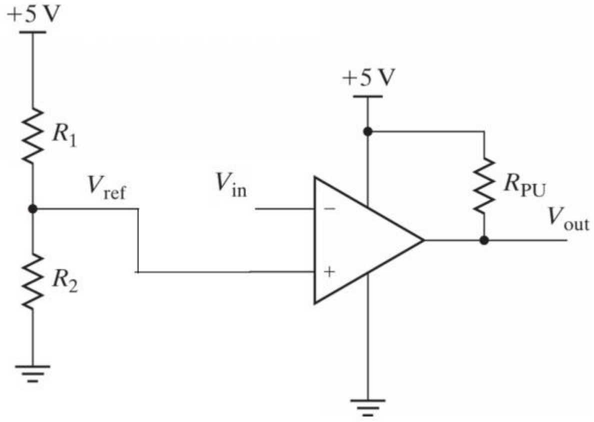


Intro to Mechatronic Design, Fig. 11.19, p. 246



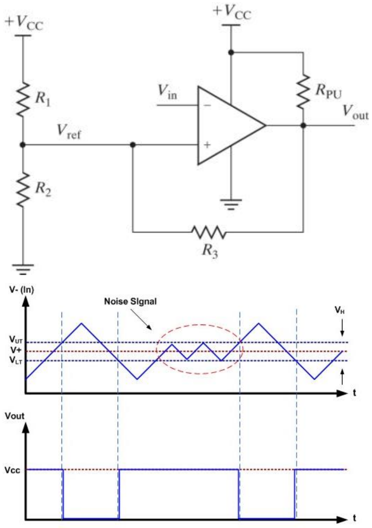
Intro to Mechatronic Design, Fig. 11.20, p. 247

Inverting Comparator



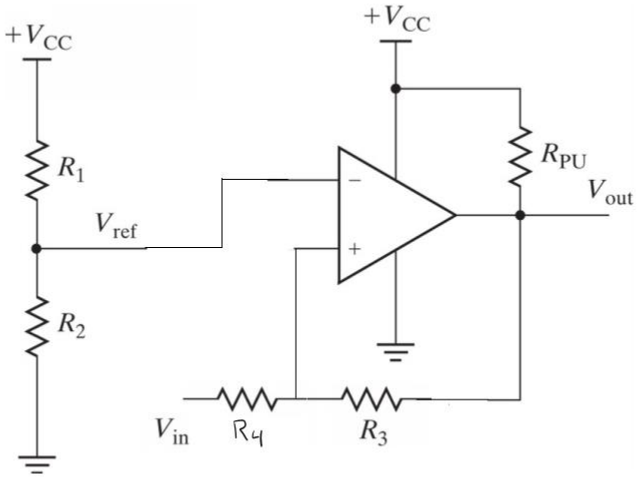
Inverting Comparator with Hysteresis

- Add hysteresis (i.e., a *change* in V_{ref} that depends on V_{out} by feeding back to the *non-inverting* terminal
  - When the input voltage *rises* to the threshold, the threshold *drops* to a *lower* value
  - When the input voltage *drops* to the threshold, the threshold is *raised* to a *higher* value



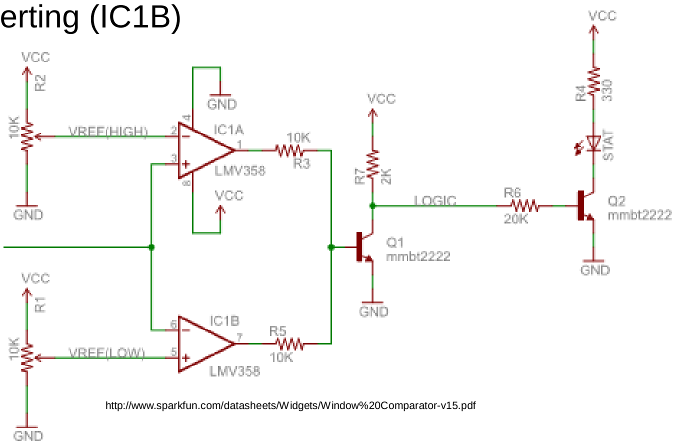
http://www.ermicro.com/blog/wp-content/uploads/2010/03/comp_10.jpg

Non-inverting comparator with hysteresis



Window comparator

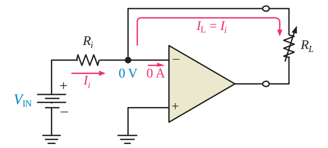
- Two comparators with two V_{refs}: $V_{refHigh}$ and V_{refLow}
  - One non-inverting (IC1A)
  - One inverting (IC1B)



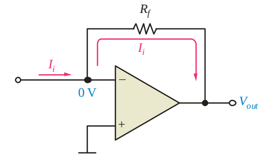
http://www.sparkfun.com/datasheets/Widgets/Window%20Comparator-v15.pdf

Summary

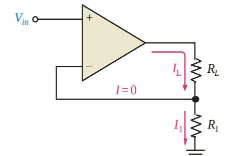
Other Op-amp Circuits



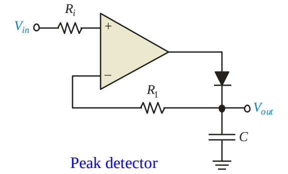
Constant-current source



Current-to-voltage converter



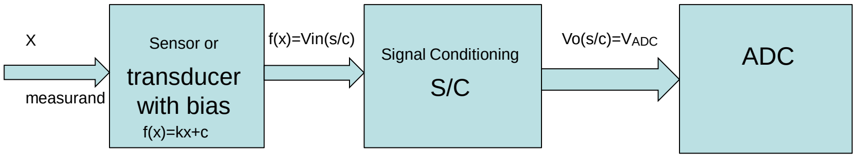
Voltage-to-current converter



Peak detector

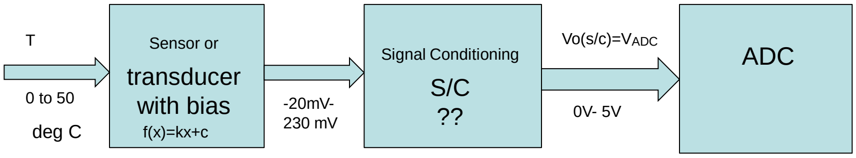
Linearization (Bias Removal)

- The signal conditioning block have two functions in this case:


X
measurand
Sensor or
transducer with bias
f(x)=kx+c
f(x)=Vin(s/c)
Signal Conditioning
S/C
Vo(s/c)=V_{ADC}
ADC

- First is to remove the bias
- Second is to make the output range of s/c block match or equal the input range of the ADC block for best system resolution

Linearization (Bias Removal)


T
0 to 50
deg C
Sensor or
transducer with bias
f(x)=kx+c
-20mV-
230 mV
Signal Conditioning
S/C
??
Vo(s/c)=V_{ADC}
0V- 5V
ADC

- Example : a sensor output changes from -20mV to +230mV as the temperature changes from 0 to 50 deg C
- Design and implement a s/c circuit such that its output matches the input range of the ADC 0-5V

x =T [C]	f(x)=Vin(sc)	Vo(sc)
0	-20mV	0
50	230mV	5

- Assuming that the sensor output is linearly dependant on the input
- Vo(sc) = a Vi(sc)+ b
- 0 = a (-20mV)+b ➔ b=0.02 a (1)
- 5V= a (230 mV)+ b (2)
- Substitute (1) in (2) and pay attention to units yields
- 5000mV =250mV x a ➔ a=20; b =0.4
- Vo(sc) =20 Vi(sc)+0.4

- Vo(sc) =20 Vi(sc)+0.4
- =20(Vi(sc)-0.02)
- The above function can be implemented in different ways such as instrumentation amplifier, difference amplifier and others

Implementation using IA

- 1+2/a=20 ==> a=2/19
- Assume Internal resistance of IA=20kΩ

then aR=(2/19)*20 kΩ = 2.105 kΩ